

# Achieving High-Accuracy Voltage (or Current) Regulation with the DCM Up to $\pm 1\%$ Regulation

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## Introduction

The DC-DC Converter Module (DCM™) provides isolation, regulation, fault protection and monitoring in a single module. Through a negative slope load line and temperature coefficient, DCM arrays implement wireless current sharing. In either single DCM circuits or in arrays, the nominal load regulation is about 5% (see the  $\%V_{OUT-LOAD}$  specification in the DCM data sheet), excluding other regulation error terms. This may not be sufficient for applications that have tight voltage regulation requirements. In those applications, an isolated analog feedback loop, such as the one shown in Figure 1, can be used to improve the load regulation performance. The circuit shown here is recommended for general use in high-accuracy applications that need to preserve the input-output isolation offered by the DCM. The circuit is applicable to single DCMs as well as arrays of up to eight units.

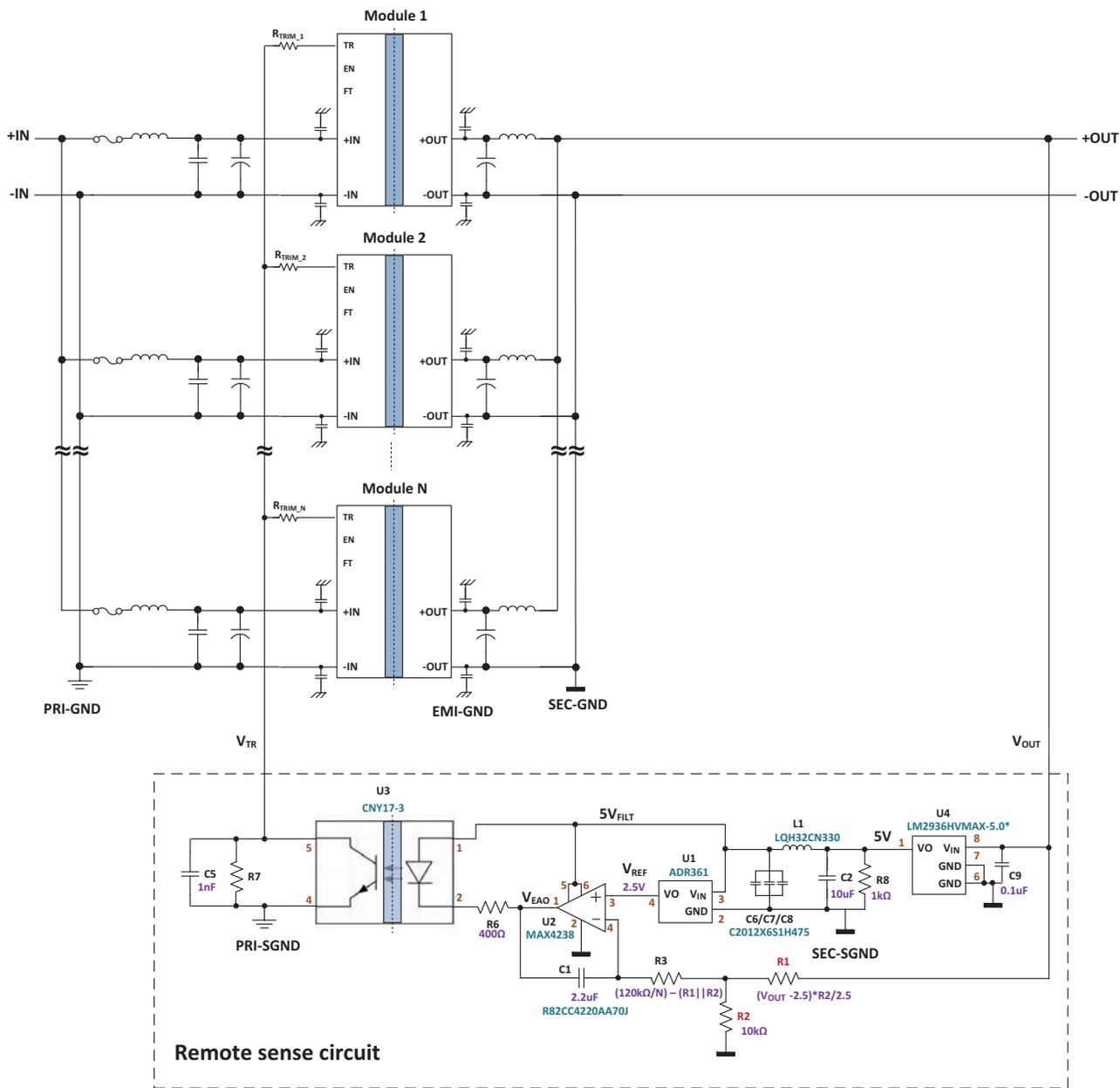
For array applications, on the primary side, after any needed differential-mode filtering, the DCMs must share a common  $-IN$  node, which is also the ground reference for the remote-sense subcircuit output. The DCM TR pins are all driven by single output of the remote-sense subcircuit, so it is important to minimize voltage differences between the various DCM  $-IN$  pins through careful layout techniques. On the secondary side, the remote-sense subcircuit senses the output voltage through the R1/R2 resistor network, compares that to a reference voltage, and converts the error voltage into a trim voltage for the whole array.

Since the DCMs are all effectively programmed to the same trim voltage, the current sharing between modules is still the same as it would be without the remote-sense circuit, as covered in [AN030: Parallel DCMs](#).

This circuit works with all ChiP™ DCM types, and achieves a regulation accuracy of  $\pm 1\%$  at all line, load, temperature and trim conditions.

# Circuit Schematic

**Figure 1**  
Remote-sense circuit  
for DCM™



\*See Table 1

## Functional Description of Remote-Sense Circuit

The output voltage is sensed through resistor network R1 and R2 relative to secondary ground SEC-SGND; the sensed voltage becomes

$$V_{OUT} \cdot \frac{R2}{R1 + R2} \quad (1)$$

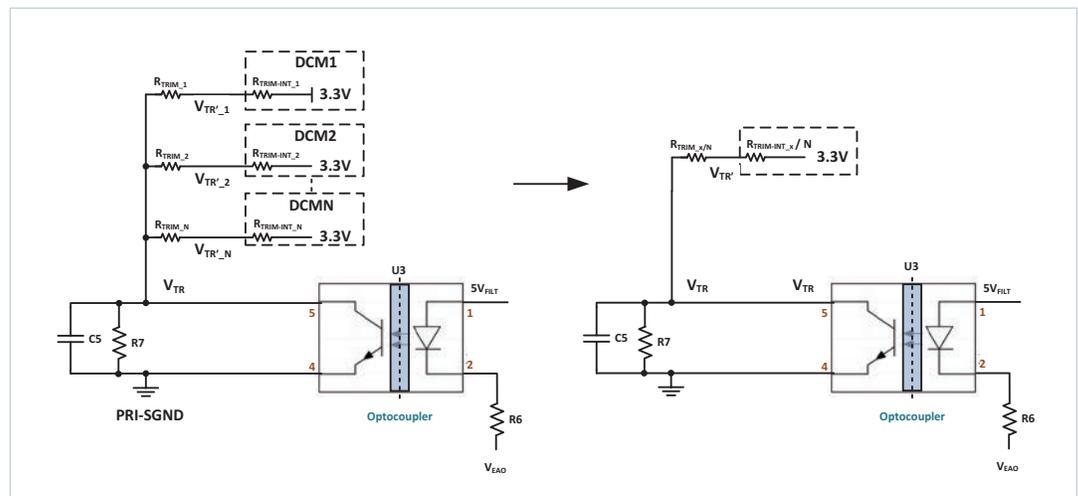
1. The sensed voltage is compared to the reference voltage  $V_{REF}$ , which in this schematic is generated by the 2.5V reference U1.

$$V_{REF} = 2.5V \quad (2)$$

If another  $V_{REF}$  voltage is preferred,  $V_{REF}$  is recommended to be between 1.5V and 3V for optimum noise immunity.

2. The difference gets accumulated by an integrating error amplifier (consisting of R3, C1 and U2), which generates  $V_{EAO}$ .
3. The difference between  $V_{EAO}$  and 5  $V_{FILT}$  drives the input of the optocoupler U3.
4. The optocoupler (U3) is used to preserve the galvanic isolation of the DCM array.
5. The output of U3 is its collector current. That current develops a voltage drop across the  $R_{TRIM\_X}$  and  $R_{TRIM-INT\_X}$  resistors and establishes the DCM™ trim pin voltages. (The  $R_{TRIM-INT\_X}$  are the internal pull-up resistors inside each DCM. Each  $R_{TRIM-INT\_X}$  pulls up to VCC, the DCM's internally generated 3.3V supply.) Figure 2 details how the trim pin voltages are generated, along with a simplified model for N DCMs in parallel. The  $R_{TRIM\_X}$  resistors are all the same nominal value, as are all of the  $R_{TRIM-INT\_X}$  resistors.

**Figure 2**  
Trim voltage generation method and its simplified model



6. If the sensed version of  $V_{OUT}$  is less than  $V_{REF}$ , the error amplifier output rises, and the drive current into the optocoupler's LED is reduced. This in turn reduces the optocoupler's (output) collector current, permitting the pull-up resistors to pull the trim voltage higher, which raises each DCMs programmed output trim voltage. Conversely, if  $V_{OUT}$  is too high, the DCM trim pin voltages are similarly driven lower, which lowers  $V_{OUT}$ .

7. R6 is chosen to set the voltage transfer ratio of the optocoupler, to ensure that it operates as expected over temperature and with age (see Appendix I).
8. R7 establishes a minimum load on the TR pins by setting the maximum trimbus voltage.
  - a. R7 must be chosen so that the maximum trim voltage will be below the TR trim enable threshold, even with no optocoupler current; some margin is needed so that trim remains enabled in the presence of noise.
  - b. The value of R7 may be further reduced, to limit the maximum trim voltage, which can be helpful in reducing overshoot during load transients and start up. For N DCMs in parallel, the trim voltage input to the DCM™,  $V_{TR\_x}$  (see Figure 2), can be calculated as:

$$V_{TR\_max} = 3.3 \cdot \frac{N \cdot R7 + R_{TRIM\_x}}{N \cdot R7 + R_{TRIM\_x} + R_{TRIM-INT\_x}} \quad (3)$$

Where  $R_{TRIM\_x} = 301\Omega$ ,  $R_{TRIM-INT\_x} = 10k\Omega$  as specified in the DCM data sheet, N is the number of DCMs in parallel.

Thus the maximum trim voltage input can be calculated as:

$$V_{TR\_max} = 3.3 \cdot \frac{N \cdot R7 + 301}{N \cdot R7 + 10301} \quad (4)$$

For example, if the trim voltage is to be limited to 3V, the value of R7 can be chosen as:

$$R7 = \frac{100k\Omega}{N} \quad (5)$$

C5 is a low-value ceramic capacitor, such as 1nF, which is used to exclude high-frequency noise from  $V_{TR}$ .

9. The bus that is used to supply U1, U2 and U3 is generated from  $V_{OUT}$ . Through this method, no external 5V power supply is needed. U4 regulates  $V_{OUT}$  to an unfiltered 5V, which is called 5V in Figure 1. This 5V then goes through the filter network (C2, L1, C6-C8) and becomes a filtered 5V, which is called 5V<sub>FILT</sub>. R8 discharges the filter capacitors when  $V_{OUT}$  is off. The output of this circuit is the 5V<sub>FILT</sub> bus that supplies U1, U2 and U3.
10. Optionally, U4/C6-C8/L1/C2/R8 can be removed from the circuit if a precision external 5V power supply with at least 50mA capability is available to drive the 5V<sub>FILT</sub> bus. The benefit of using an external 5V power supply is that it uses fewer components. The disadvantage is that if the external supply is energized before the DCMs are enabled, then the error amplifier will “wind up” to a maximum trim condition. When the DCMs are started, the system output voltage will significantly overshoot the setpoint until the integrator unwinds. When using an external 5V power supply, R7 should be chosen carefully so that  $V_{OUT}$  does not exceed the maximum voltage allowed by the application, or the DCMs should be enabled prior to energizing the external 5V supply node.

Through this method, the output voltage of the DCM™ can be trimmed to:

$$V_{OUT} = V_{REF} \cdot \frac{R1 + R2}{R2} \quad (6)$$

The maximum cut off frequency of the whole loop is 30Hz, but with CTR variance, temperature, and aging of the optocoupler, it can be as low as approximately 7.5Hz.

**Table 1**

Notes for the choice of U4

V <sub>OUT</sub>	U4 Recommendation	Comment
6V ≤ V <sub>OUT</sub> ≤ 60V	Use LM2936HVMAX-5.0 for U4	
V <sub>OUT</sub> ≤ 6V	Use an appropriate regulator for U4 so that the output voltage of U4 will be between 4V and 5.5V, or use an independent supply rail in the application	For DCM modules with a rated V <sub>OUT-NOM</sub> of 5V or 3.3V, for example.

## Component Selection

The following resources can be used to facilitate the selection of filter network components:

- Each DCM's data sheet
- [AN030: Parallel DCMs](#)
- [Powerbench Filter Design Tool](#)
- [AN023: Filter Network Design for DC-DC Converter Modules](#)

The detailed schematic of the DCM remote-sense circuit has been shown in Figure 1, with IC device types and component values. The generic components' part numbers have not been marked in the schematic. Unconnected pins have not been shown for simplicity.

The recommended components for the remote-sense circuit are summarized here (excluding the generic components):

**Table 2**

*Recommended components for remote-sense circuit*

Part ID	Type	Manufacturer Part Number	Digi-Key Part Number	Note
C1	CAP FILM 2.2μF 50V <sub>DC</sub> RADIAL	R82CC4220AA70J	399-6027-ND	Low leakage, low dielectric absorption
U1	IC V <sub>REF</sub> SERIES 2.5V TSOT23-5	ADR361BUJZ-REEL7	ADR361BUJZ-REEL7CT-ND	High precision
U2	IC OPAMP GP 1MHZ RRO SOT23-6	MAX4238AUT+T	MAX4238AUT+TDKR-ND	Low input offset voltage, low input offset current, low supply consumption, but not necessarily high bandwidth or high slew rate
U3	OPTOISO 5KV TRANS W/BASE 6SMD	CNY17-3X017T	CNY17-3X017TCT-ND	5kV isolation; Current Transfer Ratio no less than 100% @ 10mA
U4	IC REG LDO 5V 50MA 8SOIC	LM2936HV-MAX-5.0/NOPB	LM2936H-VMAX-5.0/NOPBCT-ND	See Table 1
C6/C7/C8	CAP CER 4.7μF 50V 20% X6S 0805	C2012X6S1H-475M125AC	445-7600-1-ND	
L1	IND 33μH 10% 200mA	LQH32CN330K53L	490-4062-1-ND	High precision

R1, R2 and R7 may vary according to the application and DCM™ module. Consider the following before choosing these values:

- a.  $R1/R2 = V_{OUT}/V_{REF} - 1$ ,  $V_{OUT}$  is the trimmed DCM output voltage.
- b. Choose high-accuracy resistors (up to 0.1% accuracy) for R1 and R2; their accuracy directly relates to the resultant output voltage setpoint.
- c. Choose R2 = 10kΩ; then the resistance of R1 can be calculated as:

$$R1 = \frac{V_{OUT} - 2.5}{2.5} \cdot R2$$

This will minimize current consumption and power dissipation in the divider network, while maintaining good immunity from noise and effects of bias currents from amplifier input. With R2 being fixed at 10kΩ, a high-accuracy resistor value for R1 may not be available. In that case, the nominal value of R2 can be adjusted to be within +/-10% of 10kΩ.

- d. R7 limits the maximum programmed trim for the DCMs. Use Equation (3) to determine the value of R7.

## Loop Compensation

When trim is active, the DCM TR pin provides dynamic trim control of the module's output voltage with at least 30Hz of (small signal) control bandwidth over the output voltage of the DCM converter. The phase shift at 30Hz is approximately 45°.

The whole open loop transfer function at 30Hz or below can be calculated as:

$$A(s) = A_{TR}(s) \cdot \frac{R2}{R2 + R1} \cdot \frac{1}{R3' \cdot C1 \cdot s} \cdot CTR \cdot \frac{R_{TRIM-INT-x}}{N \cdot R6} \quad (7)$$

Where CTR is the Current Transfer Ratio of the optocoupler, which is specified in the optocoupler data sheet;

$$R3' = R3 + \frac{R1 \cdot R2}{R1 + R2}$$

recall that N is the number of DCM™ modules in parallel.

For frequencies less than or equal to 30Hz, the analysis is as follows:

$A_{TR}(s)$  is the transfer function from TR to  $V_{OUT}$ , which is a constant  $A_{TR}$  at very low frequency and  $\leq A_{TR}$  at 30Hz.

$$V_{OUT} \cdot \frac{R2}{R1 + R2} = 2.5 \quad (8)$$

Rearranging the equality:

$$\frac{R2}{R2 + R1} = \frac{2.5}{V_{OUT}} \quad (9)$$

Multiplying both sides by  $A_{TR}(s)$ ,

$$A_{TR}(s) \cdot \frac{R2}{R2 + R1} = \frac{2.5 \cdot A_{TR}(s)}{V_{OUT}} \quad (10)$$

The term  $\frac{2.5 \cdot A_{TR}(s)}{V_{OUT}}$  increases with increasing trim range. For existing DCMs, the

widest trim range is -40% to 10% of  $V_{OUT\_NOM}$ . For these DCMs,  $\frac{2.5 \cdot A_{TR}}{V_{OUT\_MIN}} \approx 1$

Therefore:

$$A_{TR}(s) \cdot \frac{R2}{R2 + R1} \leq 1 \quad (11)$$

$$A(s) \leq 1 \cdot \frac{1}{R3' \cdot 2.2\mu F \cdot s} \cdot CTR \cdot \frac{10k\Omega}{N \cdot 400} \quad (12)$$

Inserting this result into Equation 7:

If R3 is chosen so that A(s) goes to 0dB at 30Hz, the whole system will have approximately 45° phase margin.

Setting A(s) to 0dB at 30Hz results in:

$$R3' = \frac{60k\Omega \cdot CTR}{N} \tag{13}$$

For the optocoupler used in the schematic, the maximum CTR is in the range of 1 to 2. So for the worst case gain, CTR = 2:

$$R3' = \frac{120k\Omega}{N} \tag{14}$$

$$R3 = \frac{120k\Omega}{N} - \frac{R1 \cdot R2}{R1 + R2} \tag{15}$$

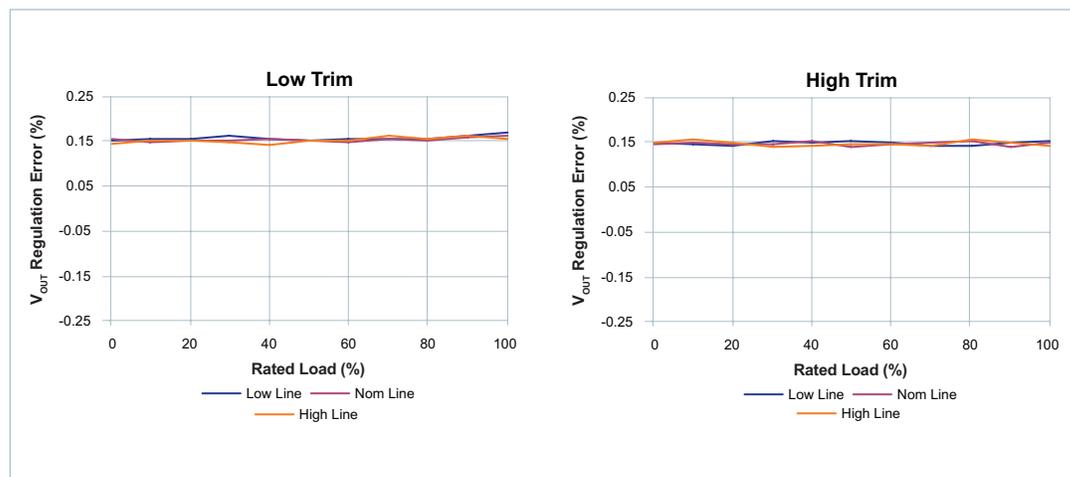
## Experimental Results (Steady State, Start Up, and Transient)

### Steady State Load Regulation

Using the DCM4623TD2H53E0T00 as an example, experimental results for a single DCM™ are shown in Figure 3; the results for an array of eight DCMs are shown in Figure 4.

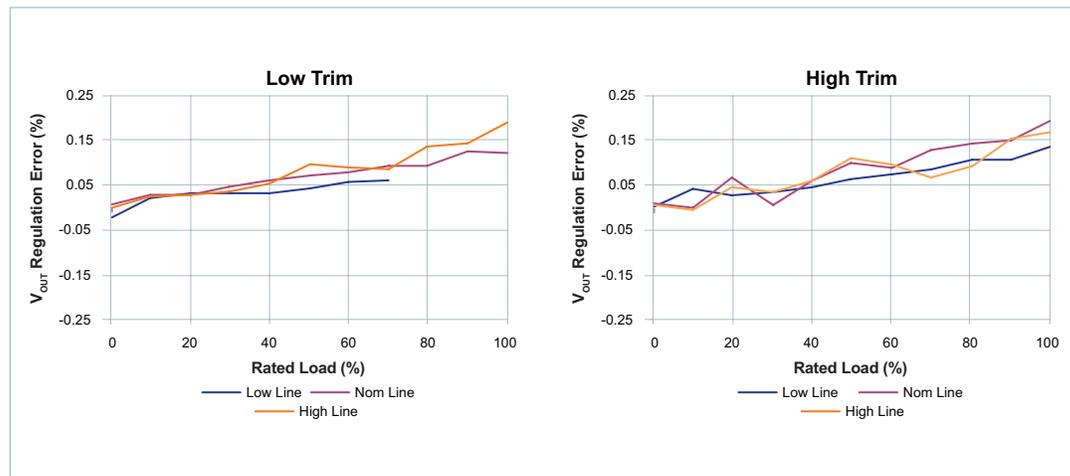
**Figure 3**

The experimental results for single DCM4623TD2H53E0T00 with this remote-sense circuit



**Figure 4**

Experimental results for an 8-up DCM4623TD2H53E0T00 array with this remote-sense circuit



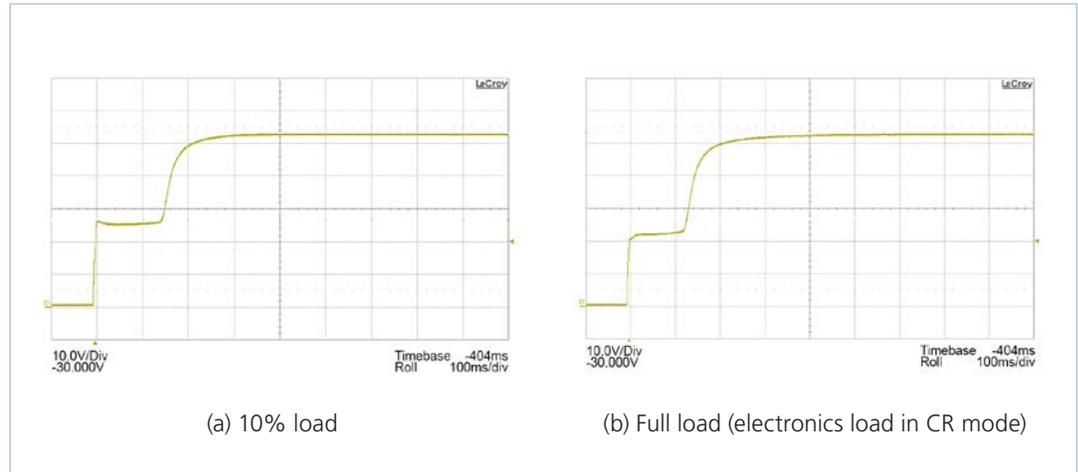
## Start Up

Typical start-up waveforms are shown in Figure 5 and Figure 6. During start up, once  $V_{OUT}$  reaches U4's minimum input voltage, U4 will generate the 5V bus to supply U1, U2 and U3. The waveform of the start up typically comes in two stages: in the first stage,  $V_{OUT}$  rises to the minimum trimmed  $V_{OUT}$ ; in the second stage, the circuit comes to the steady state and brings  $V_{OUT}$  to the correct trimmed value.

This circuit needs to be started up after  $V_{OUT}$  and the 5V bus have fully discharged to avoid trimming to the highest  $V_{OUT}$ .

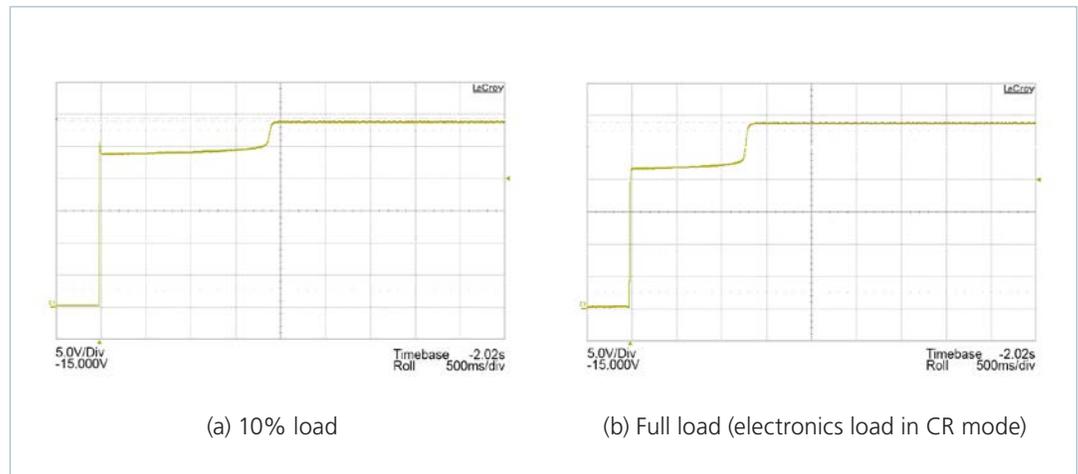
**Figure 5**

Experimental results for a single DCM4623TD2H53E0T00 (low line, maximum external  $C_{OUT}$ ) start up into high trim with this remote-sense circuit



**Figure 6**

Experimental results for a single DCM4623TD2H53E0T00 (high line, maximum external  $C_{OUT}$ ) start up into low trim with this remote-sense circuit

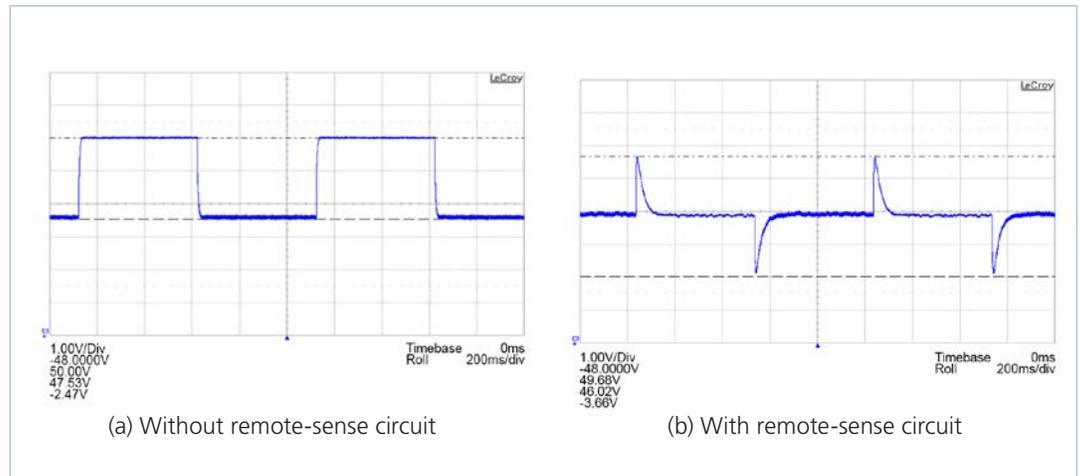


## Load Transient Response

There is a delay from the transient until the circuit reaches the corrected output voltage, which is due to the limited bandwidth of the DCM TR pin and remote-sense circuit. Because of this narrow bandwidth, the remote-sense circuit doesn't affect the initial response to a transient. Figure 7 shows a comparison of transient response without the remote-sense circuit to the response with the remote-sense circuit in operation.

**Figure 7**

Comparison of a single DCM4623TD2H53E0T00 transient response (nominal line, nominal trim, electronic load in CC mode 10% to 100% load transient) without the remote-sense circuit and with the circuit included

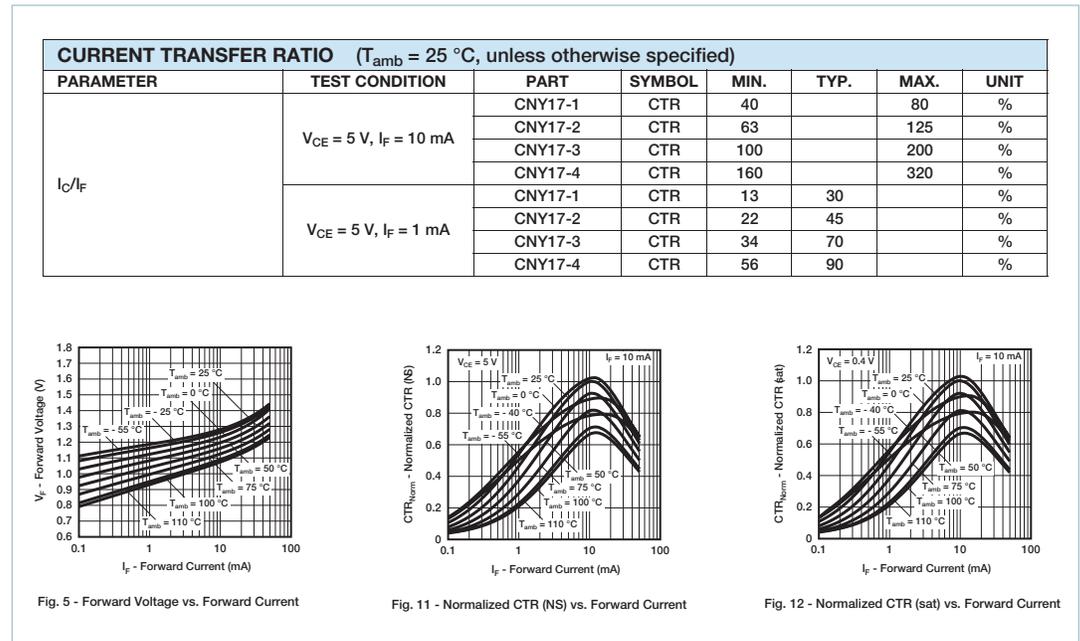


## Conclusion

Using the remote-sense circuit shown here, DCM-based voltage regulators can achieve output voltage accuracy of  $\pm 1\%$ . Within the 30Hz bandwidth of the circuit, other aspects of DCM™ operation are unchanged. This method works for any number of DCMs in parallel, up to eight.

## Appendix I. Choosing R6 to Account for CTR Variance in the CNY17-3 Over Temperature and Time

### 1. Information from Vishay CNY17 data sheet



Tables and Figures courtesy of Vishay Intertechnology, Inc.

### 2. Calculation of CNY17-3 controller current achievable over temperature and time:

- Choosing  $R6 = 400\Omega$ , a supply voltage of 4V (the lowest value specified in Table 1),  $CTR = 100\%$  and estimating the voltage drop across the optocoupler at 1.28V, the maximum forward current that the secondary side of the remote-sense circuit could have over the full temperature range is approximately  $(4V - 1.28V)/400\Omega = 6.8\text{ mA}$ .
- The next step is to find the minimum CTR at  $I_F = 6.8\text{ mA}$ , using linear interpolation on the data in the table for  $I_F = 1\text{ mA}$  and  $I_F = 10\text{ mA}$ . This results in a minimum CTR of  $((10\text{ mA} - 6.8\text{ mA}) \cdot 34\% + (6.8\text{ mA} - 1\text{ mA}) \cdot 100\%)/(10\text{ mA} - 1\text{ mA}) = 76.5\%$  at  $25^{\circ}\text{C}$
- From the Normalized CTR curves above, CTR could decrease to 60% of its peak value over temperature, which is  $76.5\% \cdot 60\% = 45.9\%$
- From Vishay reliability data, CTR is reduced by 15% over 8000 operation hours, giving  $CTR = 45.9\% \cdot (1 - 15\%) = 39\%$
- Thus the collector current will be at least  $6.8\text{ mA} \cdot 39\% = 2.65\text{ mA}$ , to ensure proper operation with aging.
- Since  $3.3V - (2.65V \cdot 1.25) = -0.01V < 0V$ , this will result in a trim voltage close to 0V, which is sufficient to drive all DCMs to trim low.
- When the forward current is small, the CNY17-3 will be able to drive all DCMs to high trim, so high trim is achievable for any choice of R6.

Thus  $R6 = 400\Omega$  should be a valid choice for this circuit to work over temperature and time, from single DCMs through arrays of eight DCMs.

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## Appendix II. Current Regulation

If current regulation is needed instead of voltage regulation, with some modifications, the remote-sense circuit can be adapted to regulate a constant-current output.

Instead of sensing the output voltage with R1 and R2, a shunt resistor is used to measure the output current. The voltage across the shunt resistor is sensed with an additional differential amplifier stage, which feeds R3. R1 and R2 are not present, since the current signal scaling is accomplished by current sense amplifier. The rest of the circuit is unchanged. A typical schematic with the current sense sub-circuit is shown in Figure 8.

Notice that current regulation needs to be limited to the minimum rated output current ( $I_{OUT}$ ) of the DCM, to avoid interfering with the DCM's operational current limit and cause issues.

In applications such as battery charging, the actual  $V_{OUT}$  can be different from the trimmed voltage of the DCM. Additional considerations may be needed:

1. The DCM has a minimum  $V_{OUT}$  before it might detect output under voltage. For example, the DCM would not be able to charge a battery whose voltage is below  $V_{OUT\_UVP}$ .
2. The DCM current capability is reduced when the DCM is trimmed higher than nominal (regardless of the actual  $V_{OUT}$ ), so the output current from the system should be no higher than  $n \cdot (\text{Rated } P_{OUT/MAXIMUM} / V_{OUT-TRIMMING})$  to avoid entering current limit.

The transfer function between the output current  $I_{OUT}$  and the sense voltage  $V_{SENSE}$  in Figure 8 is:

$$V_{SENSE} = I_{OUT} \cdot R8 \cdot R9 \cdot Gm \quad (16)$$

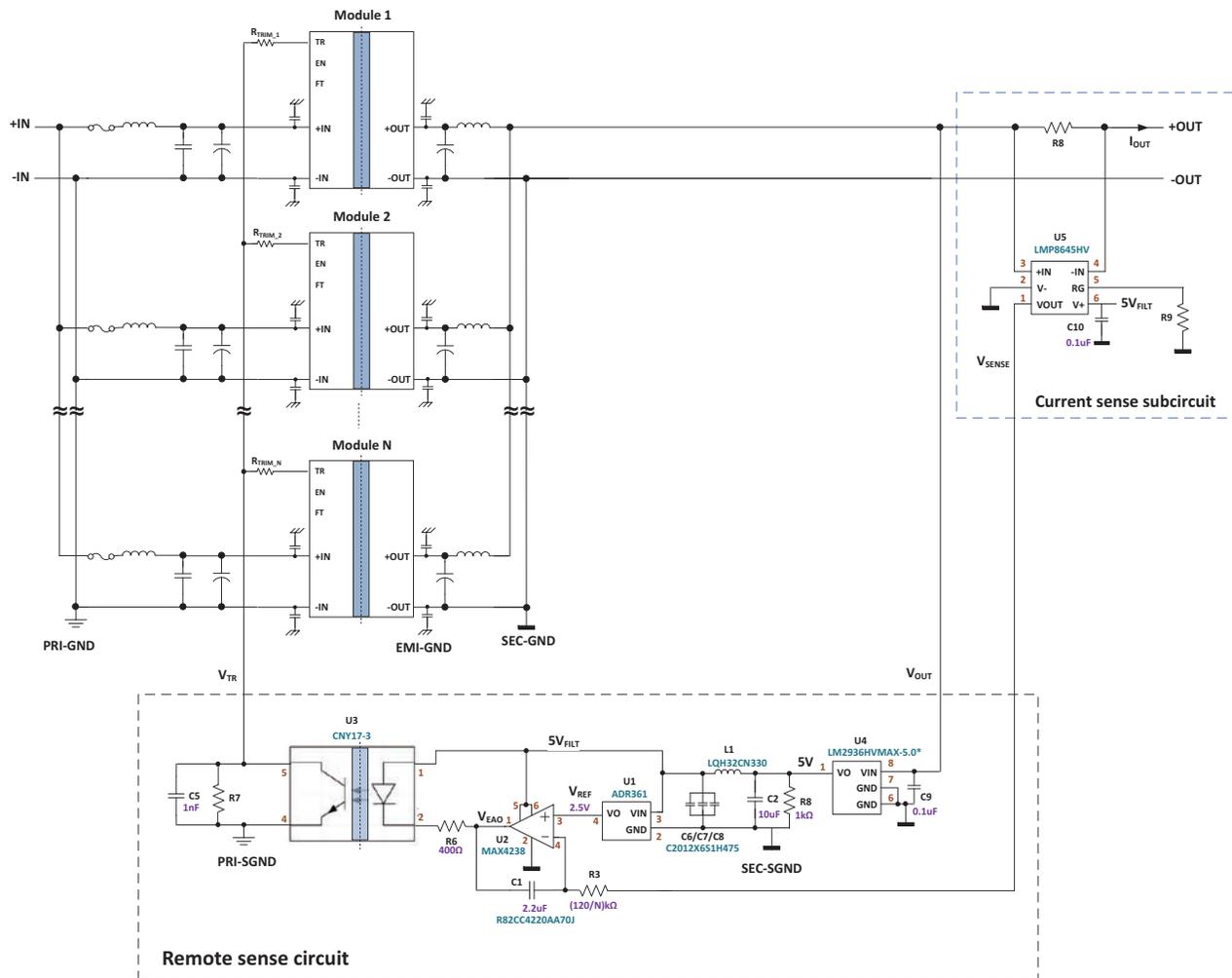
With an LMP8645HV, the typical  $Gm$  is  $200\mu A/V$ .

Through this method, the total output current of the DCMs can be trimmed to:

$$I_{OUT} = V_{REF} \cdot \frac{I}{R8 \cdot R9 \cdot Gm} \quad (17)$$

**Figure 8**

Remote-sense circuit for DCM for current regulation with single current-sense shunt



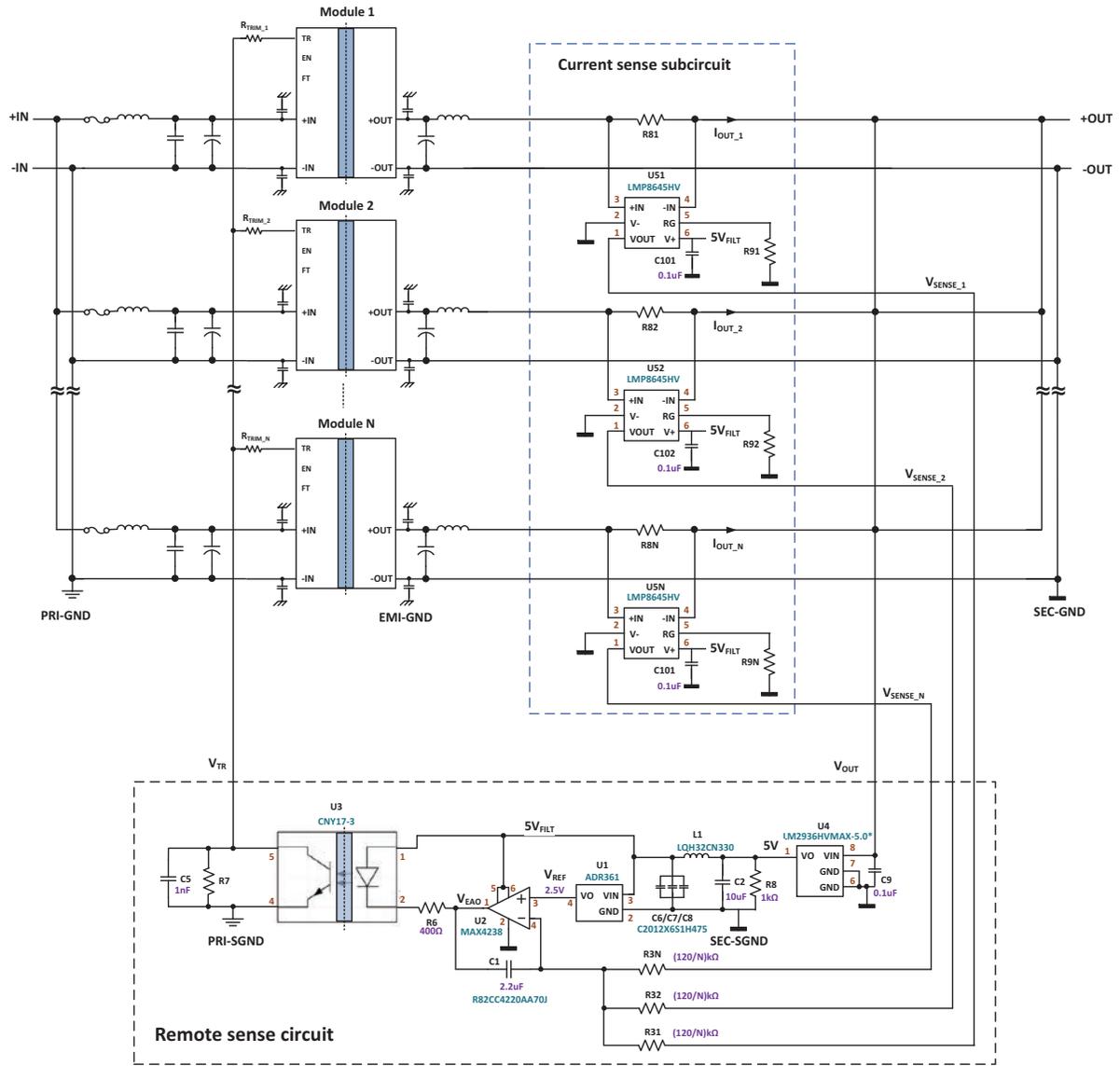
\*See Table 1

In high-current applications, individual current sense resistors for each DCM output may be preferred (as shown in Figure 9) over using a single high-dissipation current sense resistor for the entire DCM array. With  $R_{81}, R_{82}, \dots, R_{8N}$  all equal to  $R_8$ , and  $R_{91}, R_{92}, \dots, R_{9N}$  all equal to  $R_9$ , the total output current of the DCMs can be trimmed to:

$$I_{OUT} = V_{REF} \cdot \frac{I}{R_8 \cdot R_9 \cdot G_m} \quad (18)$$

**Figure 9**

Remote-sense circuit for DCM  
for current regulation with  
individual current-sense shunts



\*See Table 1

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